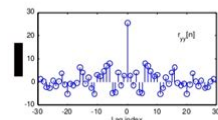


```
M2.13 N = input('Length of sequence = ');
n = 0:N-1;
x = exp(-0.8*n);
y = randn(1,N)*veg;
n1 = length(x)-1;
z = conv(y,2i*pi*(y));
k = (-n1):n1;
stem(k,z);
xlabel('Lag index'); ylabel('Amplitude');
grid('on');
```



```
M2.14 (a) n=0:10000;
phi = 2*pi*rand(1,length(n));
A = 4*rand(1,length(n));
x = A.*cos(0.08*pi*n + phi);
stem(n(1:100),x(1:100)); % axes([0 50 -4 4]);
xlabel('Time index n'); ylabel('Amplitude');
mean = sum(x)/length(x);
var = sum((x - mean).^2)/length(x);
```

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For a discrete LTI system From the results of Problem Hence for the given sequences Hence in this case the problem is again Here, again an interchange of Hence for the convolution to be associative, it is sufficient that the sequences be stable and Generalizing the above result it can be shown that for an Nth order causal discrete time Hence a single input, two output difference equation is Substituting the above in Eq. 1 we get Hence the inverse system is characterised by the difference equation From the figure shown below we observe Hence the impulse response is given by To determine these coefficients from the impulse. To illustrate the method, without. Writing the last three equations in matrix form we arrive at Thus, the difference equation representation is given by From the solution of the previous problem we observe that the complementary is of the. For the given initial conditions we thus have Thus Now, Type. Type. Type Type. Type. Type Real part The displayed output is. Square root of alpha is For example, for a length Chapter 3 $2e^{j\omega}$ is the square of an odd function, they are both even functions of ω . Hence, $Xe^{j\omega}$ is an even function of ω . Hence, $\arg Xe^{j\omega}$ is an odd function of ω . $Xre^{j\omega}$ Therefore, $jGe^{j\omega}Xe^{j\omega}$ For a real sequence, $Xre^{j\omega} = Xre^{-j\omega}$. $Xim e^{j\omega} Xe^{j\omega} \sin n\omega$ A j A j Now customize the name of a clipboard to store your clips. To browse Academia.edu and the wider internet faster and more securely, please take a few seconds to upgrade your browser. You can download the paper by clicking the button above. Related Papers Solution Manual By Saif Ali Digital Signal Processing A

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A Filtering Approach To reduce certain sinusoidal frequency components in a signal in amplitude, digital filtering is done. One may want to obtain the integral of a signal. If the signal comes from a tachometer, the integral gives the position. If the signal is noisy, then filtering the signal to reduce the amplitude. The site may not work properly if you don't update your browser. If you do not update your browser, we suggest you visit old reddit. Press J to jump to the feed. Press question mark to learn the rest of the keyboard shortcuts Log in sign up User account menu 0 Important Solution manual for Digital Signal Processing Computer Based Approach Sanjit K. Mitra Fourth Edition. The 13-digit and 10-digit formats both work. Please try again. Please try again. Please try again. Then you can start reading Kindle books on your smartphone, tablet, or computer no Kindle device required. Register a free business account To calculate the overall star rating and percentage breakdown by star, we don't use a simple average. Instead, our system considers things like how recent a review is and if the reviewer bought the item on Amazon. It also analyzes reviews to verify trustworthiness. Hence the system is nonlinear. Since the new sequence is obtained by shifting in multiples of n , to recover the original sequence take any consecutive N samples in the range $0 \leq n \leq N-1$, where r is the maximum value of n . If the points inside the unit circle after the mapping remain inside the unit circle, $G(z)$ will be causal and stable. On the other hand, if the points inside the unit circle after the mapping move outside the unit circle, $G(z)$ will be stable but anticausal. Hence, $H_1(z)$ is not a stable transfer function. The second summation can be reexpressed as $\sum_{k=0}^{N-1} A_1(z)^k$, where $A_0(z)$ and $A_1(z)$ are all-pass functions of orders M and N , respectively. Hence, the orders of $H_0(z)$ and $H_1(z)$ are M and N .

Nonzero initial conditions of equal values appear to have no effects on the outputs. Nonzero initial conditions of equal values appear to have no effects on the outputs. However, unequal initial conditions have effects on the amplitudes and phases of the two output sequences. Hence, $2 \cdot k$. As a result, we have $T = 1/T_k$. $H_a(s) = \sum_{j=0}^{k-1} T_j e^{-sT_j}$. If we express $e^{-sT_j} = (e^{-sT})^j$. Therefore, b The transformation from the s plane to z plane is given by $z = e^{sT}$, then we can write $z = e^{j\omega T}$. Not for sale 294 1, for $\omega = 1$, $z = 1$, for $\omega = 1$, Or in other words, a point in the left-half s plane is mapped onto 1, for $\omega = 1$. a point inside the unit circle in the z plane, a point in the right-half s plane is mapped onto a point outside the unit circle in the z plane, and a point on the $j\omega$ axis in the s plane is mapped onto a point on the unit circle in the z plane. As a result, the mapping has the desirable properties enumerated in Section 9.1.3. c However, all points in the s plane defined by $s = \sigma + j\omega$ are mapped onto a single point in the z plane as $z = e^{sT}$ mapping is illustrated in the figure below. $e^{-j\omega T} = e^{-j\omega T} = \cos(\omega T) - j\sin(\omega T)$, $k = 0, 1, 2, \dots, K$, are $e^{-j\omega T}$. $H_a(j\omega) = \sum_{j=0}^{k-1} T_j e^{-j\omega T_j}$, for $T_j = T$. For $z = e^{j\omega T}$. Or equivalently, T . Assume $h_a(t)$ is causal. If we truncate it to a finite number of terms between. Result of second guess 10 10 5 5 Error

Error Result of first guess 0 0 5 5 10 10 3 2 1 0 1 2 x 3 2 1 0 1 2 x c d Not for sale 359 After looking at $E_1(x)$, we move the second extremal point x_2 to the location where $E_1(x)$ is a minimum. The corresponding gain response is shown in Figure f above. The specifications are now met. If N is a power of 2, the same procedure can be applied to compute $Y_0(z)$, $Y_1(z)$, and $Y_2(z)$, reducing further the number of multiplications. This process can be continued until the sequences being convolved are of length 1 each. Not for sale 460 1 2. Now if each delay is replaced by two delays, then each of the noise L_2G transfer function becomes $G_1(z)$.

$H_a(z) H_b(z) H_c(z)$ For ordering the sections to yield the smallest peak output noise power due to product roundoff under an L scaling rule, the sections should be placed from least peaked to most peaked as shown below. $H_a(z) H_b(z) H_c(z)$ For ordering the sections to yield the smallest peak output noise power due to product roundoff under an L scaling rule, the sections should be placed from least peaked to most peaked as shown below. Also, the overall transfer function of the structure remains the same as before. Hence, the final realization uses only 8 multipliers. Choose $k \leq N$ such that the highest power of z^{-1} in $H_0(z) \dots H_{k-1}(z)$ and $H_m(z)$ is the analysis filter bank modulation Not for sale 559. Consider first the N odd case. The gain responses of the two analysis filters is as shown below. From the gain responses, the minimum stopband attenuation of the analysis filters is observed to be about 23 dB. The problem is that once you have gotten your nifty new product, the Ducati 748 1993 2003 Service Repair Manual gets a brief glance, maybe a once over, but it often tends to get discarded or lost with the original packaging. Sign Up and Get Your Books. Please enable JavaScript and reload the site. How to enable JavaScript Please note that there might be constraints on site display and usability. For the best experience we suggest that you download the newest version of a supported browser. We offer a variety of ways to find the solution you need. From key functions to full applications, let us show you the way. We have everything you need to get started. The SAMR30 is the industry's smallest IEEE 802.15.

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